EE 508 Lecture 23

Filter Synthesis Strategies

- Integrators

Review from last time

Sensitivity Comparisons

Consider 5 second-order lowpass filters

(all can realize same $T(s)$ within a gain factor)

Bridged-T Feedback Community Co

$b)$ + KRC (a Sallen and Key filter) **Review from last time**

How do these five circuits compare?

- a) From a passive sensitivity viewpoint?
	- If Q is small
	- If Q is large

b) From an active sensitivity viewpoint?

- If Q is small
- If Q is large
- If τ $ω_0$ is large

Comparison: Calculate all ω_0 and Q sensitivities

Consider passive sensitivities first

a) – Passive RLC

Case b1 : +KRC Equal R, Equal C

$$
\omega_{0} = \sqrt{\frac{1}{R_{1}R_{2}C_{1}C_{2}}}
$$
\n
$$
Q = \sqrt{\frac{1}{R_{1}R_{2}C_{1}C_{2}}} \sqrt{\frac{1}{R_{2}C_{2}} + \sqrt{\frac{R_{2}C_{2}}{R_{2}C_{1}}} - K\sqrt{\frac{R_{1}C_{1}}{R_{2}C_{2}}}}
$$
\n
$$
S_{R_{1}}^{\omega_{0}} = S_{R_{2}}^{\omega_{0}} = S_{C_{1}}^{\omega_{0}} = S_{C_{2}}^{\omega_{0}} = -\frac{1}{2}
$$
\n
$$
S_{R_{2}}^{\omega_{0}} = Q - \frac{1}{2}
$$
\n
$$
S_{R_{2}}^{\omega_{0}} = -Q + \frac{1}{2}
$$
\n
$$
S_{C_{1}}^{\omega_{0}} = 2Q - \frac{1}{2}
$$
\n
$$
S_{C_{2}}^{\omega_{0}} = -2Q + \frac{1}{2}
$$
\n
$$
S_{C_{2}}^{\omega_{0}} = -2Q + \frac{1}{2}
$$
\n
$$
S_{C_{2}}^{\omega_{0}} = -2Q + \frac{1}{2}
$$
\n
$$
S_{C_{2}}^{\omega_{0}} = 3Q - 1
$$

If Q_N=10 in +KRC filter, what happens to Q if R₁ increases by 1%? By 10%?

$$
\mathbf{S}_{R_1}^Q = Q - \frac{1}{2}
$$

$$
S_{R_1}^Q = Q - \frac{1}{2}
$$

\n
$$
\frac{\Delta R_1}{R_1} = 0.01
$$

\n
$$
\frac{\Delta Q}{Q} \approx S_{R_1}^Q \bullet \frac{\Delta R_1}{R_1} \approx \left(Q - \frac{1}{2}\right)(0.01) = 9.5 \bullet 0.01 = 0.095
$$

\n
$$
Q_{PREDICT} = 10^*(1 + 0.095) = 10.95
$$

\n
$$
\frac{\Delta R_1}{R_1} = 0.1
$$

\n
$$
\frac{\Delta Q}{Q} \approx S_{R_1}^Q \bullet \frac{\Delta R_1}{R_1} \approx \left(Q - \frac{1}{2}\right)(0.01) = 9.5 \bullet 0.1 = 0.95
$$

$$
Q_{PREDICT} = 10*(1+0.095) = 10.95
$$

$$
Q_{\text{ACTUAL}} = 11.04
$$

$$
Q_{N} = 10 \text{ in +KRC filter, what happens to Q if R1 increases by 1%? By 10%?}
$$

\n
$$
S_{R_{1}}^{Q} = Q - \frac{1}{2}
$$

\n
$$
\frac{\Delta R_{1}}{R_{1}} = 0.01
$$

\n
$$
\frac{\Delta Q}{Q} \approx S_{R_{1}}^{Q} \cdot \frac{\Delta R_{1}}{R_{1}} \approx \left(Q - \frac{1}{2}\right)(0.01) = 9.5 \cdot 0.01 = 0.095
$$

\n
$$
Q_{PREDICT} = 10^{*}(1+0.095) = 10.95
$$

\n
$$
Q_{ACTUAL} = 11.04
$$

\n
$$
\frac{\Delta R_{1}}{R_{1}} = 0.1
$$

\n
$$
\frac{\Delta Q}{Q} \approx S_{R_{1}}^{Q} \cdot \frac{\Delta R_{1}}{R_{1}} \approx \left(Q - \frac{1}{2}\right)(0.01) = 9.5 \cdot 0.1 = 0.95
$$

\n
$$
Q_{PREDICT} = 10^{*}(1+0.95) = 19.5
$$

\n
$$
Q_{ACTUAL} = 105
$$

\n
$$
Q_{ACTUAL} = 105
$$

\n
$$
R_{R_{1}} = 0.1
$$

\n
$$
Q_{ACTUAL} = 105
$$

\n
$$
Q_{RCTUAL} = 105
$$

\n
$$
Q_{RSTUAL} = 105
$$

Sensitivity analysis quite useful if $\:\frac{\Delta x}{\ldots}$ is small but not accurate when $\frac{\Delta x}{\ldots}$ is large $\mathbf x$ and $\mathbf x$ and

Effects of R_1 variations on +KRC Filter

 \sim γ $S_{R_1}^Q = Q - \frac{1}{2}$

Case b2 : +KRC Equal R, K=1

=

$$
\omega_0 = \sqrt{\frac{1}{R_1 R_2 C_1 C_2}}
$$
\n
$$
Q = \sqrt{\frac{1}{R_1 R_2 C_1 C_2}}
$$
\n
$$
Q = \sqrt{\frac{1}{R_2 C_1} + \sqrt{\frac{R_2 C_2}{R_1 C_1}} + \sqrt{\frac{R_1 C_2}{R_2 C_1}} - K\sqrt{\frac{R_1 C_1}{R_2 C_2}}}
$$

$$
S_{R_1}^{\omega_0} = S_{R_2}^{\omega_0} = S_{C_1}^{\omega_0} = S_{C_2}^{\omega_0} = -\frac{1}{2}
$$
\n
$$
S_{R_1}^{\omega} = 0
$$
\n
$$
S_{R_2}^{\omega} = 0
$$
\n
$$
S_{C_1}^{\omega} = \frac{1}{2}
$$
\n
$$
S_{C_1}^{\omega} = \frac{1}{2}
$$
\n
$$
S_{C_2}^{\omega} = -\frac{1}{2}
$$
\n
$$
S_{C_2}^{\omega} = -\frac{1}{2}
$$
\n
$$
S_{C_1}^{\omega} = 2Q^2
$$
\n
$$
S_{C_2}^{\omega} = 2Q^2
$$
\n
$$
S_{C_1}^{\omega} = 2Q^2
$$
\n
$$
S_{C_2}^{\omega} = 2Q^2
$$

1

2

c) Bridged T Feedback

$$
\omega_0 = \sqrt{\frac{1}{R_1 R_2 C_1 C_2}}
$$
\n
$$
Q = \sqrt{\frac{1}{\sqrt{C_2}} \left(\sqrt{\frac{R_1}{R_1}} + \sqrt{\frac{R_2}{R_1}} + \sqrt{\frac{R_1 R_2}{R_1}} \right)}
$$

For $R_1=R_2=R_3=R$

$$
\mathbf{S}_{R_3}^{\omega_0}=0
$$

$$
\omega_0 = \frac{3Q}{RC_1}
$$

$$
Q = \frac{1}{3} \sqrt{\frac{C_1}{C_2}}
$$

d) 2 integrator loop

$$
\omega_0 = \sqrt{\frac{R_4}{R_3} \frac{1}{R_0 R_2 C_1 C_2}} \qquad \qquad Q = \frac{R_0}{\sqrt{R_0 R_2}} \sqrt{\frac{C_2}{C_1}}
$$

For: $R_0 = R_1 = R_2 = R \qquad C_1 = C_2 = C \qquad R_3 = R_4$

$$
S_{R_1}^{\omega_0} = S_{R_2}^{\omega_0} = S_{R_3}^{\omega_0} = S_{C_1}^{\omega_0} = S_{C_2}^{\omega_0} = -\frac{1}{2}
$$
\n
$$
S_{R_1}^{\omega} = S_{R_2}^{\omega} = S_{R_3}^{\omega} = S_{C_1}^{\omega} = -\frac{1}{2}
$$
\n
$$
S_{R_4}^{\omega} = S_{C_2}^{\omega} = \frac{1}{2}
$$
\n
$$
S_{R_4}^{\omega} = S_{C_2}^{\omega} = \frac{1}{2}
$$
\n
$$
S_{R_0}^{\omega} = 1
$$
\n
$$
S_{R_0}^{\omega} = 0
$$
\n
$$
S_{R_0}^{\omega} = 0
$$

1

 $\mathsf{R}_{\text{\tiny Q}}$

R

d) -KRC passive sensitivities

$$
\omega_0 = \sqrt{\frac{1 + (R_1/R_3)(1 + K) + (R_1/R_4)(1 + R_2/R_3 + R_2/R_1)}{R_1R_2C_1C_2}}
$$

$$
Q = \frac{\sqrt{\frac{1 + (R_1/R_3)(1 + K) + (R_1/R_4)(1 + R_2/R_3 + R_2/R_1)}{R_1R_2C_1C_2}}}{\left(1 + \frac{R_1}{R_3}\right)\left(\frac{1}{R_1C_1}\right) + \left(1 + \frac{C_2}{C_1}\right)\left(\frac{1}{R_2C_2}\right) + \left(\frac{1}{R_4C_2}\right)}
$$

How do active sensitivities compare? $S_{\perp}^{\omega_{o}} = ? \qquad S_{\perp}^{\omega_{e}} = ?$ Recall $S_x^f = \frac{\partial f}{\partial x} \frac{x}{f}$ So $\frac{\Delta f}{f}$ \sim $\frac{\Delta x}{x}$ \int_{x}^{f} but if X is ideally O , not useful $\Delta \frac{x}{t} = \frac{\partial x}{\partial t}$ $\frac{2}{\sigma f}$ = $\Delta_x^{\frac{1}{\sigma}}$ $\frac{2x}{f}$

Where we are at with sensitivity analysis:

Considered a group of five second-order filters

Passive Sensitivity Analysis

- Closed form expressions were obtained for ω_0 and Q
- Tedious but straightforward calculations provided passive sensitivities directly from the closed form expressions $\textcircled{?'}$??

Active Sensitivity Analysis

• Closed form expressions for ω_0 and Q are very difficult or impossible to obtain \mathbb{C}^3

If we consider higher-order filters

Passive Sensitivity Analysis

• Closed form expressions for ω_0 and Q are very difficult or impossible to obtain for many useful structures

Active Sensitivity Analysis

• Closed form expressions for ω_0 and Q are very difficult or impossible to obtain (1)

Need some better method for obtaining sensitivities when closed-form expressions are difficult or impractical to obtain or manipulate !!

Relationship between pole sensitivities and ω_0 and Q sensitivities

Relationship between active pole sensitivities and ω_0 and Q sensitivities

Define $D(s)=D_0(s)+t D_1(s)$ (from bilinear form of T(s))

Theorem: $\Delta p \cong \tau \boldsymbol{\mathit{s}}_{\tau}^{\textit{p}}$ Theorem: $\Delta \alpha \cong \tau \mathsf{Re}\big(\mathfrak{s}^{\scriptscriptstyle\mathsf{p}}_{\scriptscriptstyle \tau} \big)$. $\Delta \beta \cong \tau$ $\mathsf{Im}\bigl({\boldsymbol{\mathit{s}}_\iota^r}\bigr)$. Recall: (p) (s) -D₁(p $\vert_{\mathsf{s}=\mathsf{p},\mathsf{T}=0}$ $\mathcal{D}_\tau^{\star} = \frac{1}{\partial D(s)}$ $\partial \mathsf{s}$ **p s**

Theorem:

$$
\frac{\Delta\omega_0}{\omega_0} \approx \frac{1}{2Q} \frac{\Delta\alpha}{\omega_0} + \sqrt{1 - \frac{1}{4Q^2}} \frac{\Delta\beta}{\omega_0} \qquad \frac{\Delta Q}{Q} \approx -2Q \left(1 - \frac{1}{4Q^2}\right) \frac{\Delta\alpha}{\omega_0} + \sqrt{1 - \frac{1}{4Q^2}} \frac{\Delta\beta}{\omega_0}
$$

Claim: These theorems, with straightforward modification, also apply to other parameters (R, C, L, K, ...) where, ${\mathsf D}_0({\mathsf s})$ and ${\mathsf D}_1({\mathsf s})$ will change since the parameter is different

Second-Order Low-Pass Networks

conducture Bridged T Feedback

Table 10-3 Infinite-gain Realization (see Fig. 10-10b)

Equal-R

$$
\omega_{*} = \frac{1}{R\sqrt{C_{1}C_{2}}}; \qquad Q = \frac{1}{3}\sqrt{\frac{C_{1}}{C_{4}}}
$$
\n
$$
\frac{V_{*}}{V_{i}} = -\frac{\omega_{*}^{2}}{x^{2} + s\frac{\omega_{*}}{Q} + \omega_{*}^{2} + \frac{s}{GB}\left[s^{2} + s\omega_{*}\left(3Q + \frac{1}{Q}\right) + 2\omega_{*}^{2}\right]} \qquad \left(\omega_{*} \ll \frac{\omega_{*}}{2Q}\right)
$$
\n
$$
-\frac{\Delta\alpha}{\omega_{*}} \approx \frac{\omega_{*}}{GB}, \qquad \frac{\Delta\beta}{\omega_{*}} \approx -\frac{1}{2}\frac{3Q - \frac{1}{Q}}{\sqrt{1 - \frac{1}{4Q^{2}}}}\frac{\omega_{*}}{GB}
$$
\n
$$
\frac{\Delta\omega_{*}}{\omega_{*}} \approx -\frac{3Q}{2}\frac{\omega_{*}}{GB}, \qquad \frac{\Delta Q}{Q} \approx \frac{Q}{2}\frac{\omega_{*}}{GB}
$$

<u>ka kacamatan ing Kabupatèn Bandaran Pada Kabupatèn Bandaran Kabupatèn</u>

Fig. 10-12 Plot of upper half-plane root of

$$
s^2 + s^2 \left(3Q + \frac{1}{Q} + GB_s\right) + s_s \left(2 + \frac{GB}{Q}\right) + GB_s = 0
$$

Two integrator loop architecture

Equal-R (except R_O) and Equal-C

 $\omega_* = \frac{1}{R^{-1}}$ $Q = \frac{R_0}{R}$ $\frac{V_0}{V_1} \cong \frac{\omega_a^2 \left(\frac{2}{\text{GB}} \ s+1\right)}{s^2 + s \frac{\omega_x}{Q} + \omega_s^2 + \frac{1}{\text{GB}} \left\{4s \left[s^2 + s \omega_s \left(\frac{1}{2} + \frac{1}{Q}\right) + \frac{\omega_s^2}{4Q}\right]\right\}}$ $\left(\omega_a \ll \frac{4R_a}{2\sqrt{2}}\right)$ $-\frac{\Delta \alpha}{\omega_a} \approx 2\left(1 + \frac{1}{4Q}\right) \frac{\omega_a}{GB}, \qquad \frac{\Delta \beta}{\omega_a} \approx -\frac{\left(1 - \frac{1}{Q} - \frac{1}{4Q^2}\right)}{\sqrt{1 - \frac{1}{4Q^2}}} \frac{\omega_a}{GB}$ $rac{\Delta \omega_s}{\omega_s} \simeq -\frac{\omega_s}{GB}, \qquad \frac{\Delta Q}{Q} \simeq 4Q \frac{\omega_s}{GB}$

Two integrator loop architecture

Fig. 10-17 Plot of upper half-plane root of

$$
x_1^2 + x_2^2 \left(\frac{1}{2} + \frac{1}{Q} + \frac{GB_0}{4} \right) + x_2 \frac{1}{4Q} \left(1 + GB_0 \right) + \frac{GB_0}{4} = 0
$$

- KRC

Equal-R, Equal-C

$$
\omega_{\bullet} = \frac{\sqrt{5 + K_0}}{RC}, \qquad Q = \frac{\sqrt{5 + K_0}}{5}
$$

$$
\frac{V_e}{V_i} = -\frac{\omega_e^2 \left(1 - \frac{1}{5Q^2}\right)}{s^2 + s\frac{\omega_e}{Q} + \omega_e^2 + \frac{s}{GB} \left[s^2(25Q^2 - 4) + s\omega_e \left(20Q - \frac{3}{Q}\right) + \left(2 - \frac{1}{5Q^2}\right)\omega_e^2\right]} \left(\omega_e \ll \frac{\omega_e}{2Q}\right)
$$

$$
-\frac{\Delta\alpha}{\omega_o} \approx \frac{25Q^2}{2} \left(1 - \frac{1}{5Q^2}\right) \left(1 - \frac{6}{25Q^2}\right) \frac{\omega_o}{GB}, \qquad \frac{\Delta\beta}{\omega_o} \approx \frac{35Q}{4} \frac{\left(1 - \frac{1}{5Q^2}\right) \left(1 - \frac{6}{35Q^2}\right)}{\sqrt{1 - \frac{1}{4Q^2}}} \frac{\omega_o}{GB}
$$

$$
\frac{\Delta\omega_o}{\omega_o} \approx \frac{5Q}{2} \left(1 - \frac{1}{5Q^2} \right) \frac{\omega_o}{GB}, \qquad \frac{\Delta Q}{Q} \approx 25Q^3 \left(1 - \frac{1}{5Q^2} \right) \left(1 - \frac{7}{5Q^2} \right) \frac{\omega_o}{GB}
$$

- KRC

Substantial Differences Between Architectures

Are these passive sensitivities acceptable?

Active Sensitivity Comparisons Are these active sensitivities acceptable?

Are these sensitivities acceptable?

Passive Sensitivities:

In integrated circuits, Δ R/R and Δ C/C due to process variations can be \pm 30% or larger due to process variations

Many applications require Δ ω_{0}/ω_{0} <.001 or smaller and similar requirements on ΔQ/Q

Even if sensitivity is around $\frac{1}{2}$ or 1, variability is often orders of magnitude too large

Active Sensitivities:

All are proportional to $\tau\omega_0$

Some architectures much more sensitive than others

Can reduce τ ω_0 by making GB large but this is at the expense of increased power and even if power is not of concern, process presents fundamental limits on how large GB can be made

Observe that for the +KRC circuit, the somewhat arbitrary use of the DOF has a major impact on performance

Similar observations can be made for other structures

Challenge: Can a major improvement in performance be obtained by a more judicious use of the two free DOF for the +KRC circuit?

1. Predistortion

Design circuit so that after component shift, correct pole locations are obtained

Predistortion is generally used in integrated circuits to remove the bias associated with inadequate amplifier bandwidth

Predistortion does not help with process variations of passive components

Tedious process after fabrication since depends on individual components

Temperature dependence may not track

Difficult to maintain over time and temperature

Over-ordering will adversely affect performance

Seldom will predistortion alone be adequate to obtain acceptable performance Bell Labs did to this in high-volume production (STAR Biquad)

1. Predistortion

Design circuit so that after component shift, correct pole locations are obtained

Pole shift due to parametric variations (e.g. inadequate GB)

1. Predistortion

Design circuit so that after component shift, correct pole locations are obtained

Pre-distortion concept

1. Predistortion

Design circuit so that after component shift, correct pole locations are obtained

What can be done to address these problems? 2. Trimming

a) Functional Trimming

- trim parameters of actual filter based upon measurements
- difficult to implement in many structures
- manageable for cascaded biquads

b) Deterministic Trimming (much preferred)

- Trim component values to their ideal value Continuous-trims of resistors possible in some special processes Continuous-trim of capacitors is more challenging Link trimming of Rs or Cs is possible with either metal or switches
- If all components are ideal, the filter should also be ideal R-trimming algorithms easy to implement Limited to unidirectional trim Trim generally done at wafer level for laser trimming, package for link trims
- Filter shifts occur due to stress in packaging and heat cycling

c) Master-slave reference control (depends upon matching in a process)

- Can be implemented in discrete or integrated structures
- Master typically frequency or period referenced
- Most effective in integrated form since good matching possible
- Widely used in integrated form

Master-slave Control (depends upon matching in a process)

- Automatically adjust R (or C) in the Master Circuit to match RC to T
- Rely on matching to match RC products in Slave Circuit to T
- Matching can be very good (1% or 0.1% or better)
- But does nothing to compensate for local random variations
Master-slave Example:

- Key parameter of integrator is unity gain frequency $I_0=1/RC$
- Adjust R in Master Circuit so that $I_0=1$ at the input frequency f
- With matching, unity gain frequency of all integrators in Slave Circuit will also be 1
- May require considerable overhead to trim circuit elements
- Compensates for combined component variations and BW limitations

Master-slave Example:

- Over-ordering will limit accuracy of master-slave approach even if unity gain frequency of master circuit is precisely obtained
- Technique is often used to maintain good control of effective RC products
- Power and area overhead but Master circuit may be off most of the time to reduce power overhead

What can be done to address these problems?

3. Select Appropriate Architecture

Helps a lot

Best architectures are not known

Performance of good architectures often not good enough

What can be done to address these problems?

4. Different Approach for Filter Implementation

- • **Frequency Referenced Filters Switched-Capacitor Filters**
- • **DSP- Based Filter Implementation**
- • **Other Niche Methods**

Summary of Sensitivity Observations

- Sensitivity varies substantially from one implementation to another
- Variability too high, even with low sensitivity, for more demanding applications
- Methods of managing high variability
	- ➢ Select good structures
	- \triangleright Trimming
		- Functional

Deterministic

➢ Predistortion

In particular, for active sensitivities Useful but not a total solution

➢ Frequency Referenced Techniques

Master-Slave Control

Depends upon matching

Can self-trim or self-compensate

Switched-Capacitor Filters

AD/digital filter/D/A

➢ Alternate Design Approach Other methods

Filter Design Process

Most designs today use one of the following three basic architectures

Multiple-loop Feedback – One type shown (less popular)

Multiple-loop Feedback – Another type

$$
X = V_{IN} - X \bullet \sum_{k=1}^{n} b_{n-k} \left(\frac{I_0}{s}\right)^k
$$

$$
V_{OUT} = X \bullet \sum_{k=0}^{n} a_{n-k} \left(\frac{I_0}{s}\right)^k
$$

 $=$

$$
T\left(s\right)=\frac{\sum\limits_{k=0}^{n}a_{n-k}\left(\frac{I_{0}}{s}\right)^{k}}{1+\sum\limits_{k=1}^{n}b_{n-k}\left(\frac{I_{0}}{s}\right)^{k}}
$$

$$
T(s) = \frac{\sum_{k=0}^{n} a_{n-k} I_0^k s^{n-k}}{s^n + \sum_{k=1}^{n} b_{n-k} I_0^k s^{n-k}}
$$

•Termed the direct synthesis method

- Directly implements the coefficients in the numerator and denominator
- •Approach followed in the Analog Computers
- Not particularly attractive from an overall performance viewpoint

Will study details of all three types of architectures later

Observation: All filters are comprised of summers, biquads and integrators

Consider now the biquads

Biquad Filters Design Considerations

Several different Biquads were considered and other implementations exist

Floating Nodes

A node in a circuit is termed a floating node if it is not an output node of a ground-referenced voltage-output amplifier (dependent or independent), not connected to a ground-referenced voltage source, or not connected to a ground-referenced null-port

Parasitic Capacitances on Floating Nodes

Parasitic capacitances ideally have no affect on filter when on a non-floating node but directly affect transfer function when they appear on a floating node

Parasitic capacitances are invariably large, nonlinear, and highly process dependent in integrated filters. Thus, it is difficult to build accurate integrated filters if floating nodes are present

Generally avoid floating nodes, if possible, in integrated filters

Infinite Gain Amplifiers

- Integrator-based biquads all involve two integrators in a loop
- All integrator-based biquads discussed have no floating nodes
- Most biquads in integrated filters are based upon two integrator loop structures
- The summers are usually included as summing inputs on the integrators
- The loss can be combined with the integrator to form a lossy integrator
- Performance of the minor variants of the two integrator loop structures are comparable

Observation: All filters are comprised of summers, biquads and integrators

And biquads usually made with summers and integrators

Integrated filter design generally focused on design of integrators, summers, and amplifiers (Op Amps)

Will now focus on the design of integrators, summers, and op amps

Basic Filter Building Blocks

(particularly for integrated filters)

- Summers
- Operational Amplifiers

Integrator Characteristics of Interest

$$
X_{IN} = \frac{I_0}{s} \qquad \frac{X_{OUT}}{S}
$$
\n
$$
I(s) = \frac{I_0}{s}
$$

Properties of an ideal integrator:

$$
|\mathbf{I}(j\omega)| = \frac{\mathbf{I}_0}{\omega}
$$

$$
\angle \mathbf{I}(j\omega) = -90^\circ
$$

$$
|\mathbf{I}(j\mathbf{I}_0)| = 1
$$

Gain decreases with 1/ω

Phase is a constant -90^o

Unity Gain Frequency = I_0

How important is it that an integrator have all 3 of these properties?

Integrator Characteristics of Interest

How important is it that an integrator have all 3 of these properties?

Consider a filter example:

Band edges proportional to I_0 Phase critical to make Q expression valid

In many (most) applications it is critical that an integrator be very nearly ideal

$$
x_1^2 + x_2^2 \left(\frac{1}{2} + \frac{1}{Q} + \frac{GB_2}{4} \right) + x_2 \frac{1}{4Q} \left(1 + GB_2 \right) + \frac{GB_2}{4} = 0
$$

1 $\overline{\text{RCS}}$ $I_0 = \frac{1}{R}$

 $=$ $\overline{\text{RC}}$

Inverting Active RC Integrator

Are there other integrator structures?

Termed an OTA-C or a gm-C integrator

Are there other integrator structures?

Termed a TA-C integrator

Termed MOSFET-C integrator

C

Are there other integrator structures?

- Output current is independent of Z_1
- Thus output impedance is ∞ so provides current output

Termed active RC current-mode integrator

There are other useful integrator structures (some will be introduced later)

There are many different ways to build an inverting integrator

Many different types of functionality from basic inverting integrator Same modifications exist for other integrator architectures

Integrator-Based Filter Design

Are new integrators still being invented?

Oct 16 2018

- 51 9.063.789 T Hybrid cloud integrator plug-in components
- 52 9,061,592 T System and method for detecting power integrator malfunction
- 53 9.054.731 T Integrator output swing reduction
- 54 9.039.190 T Projector having integrator with greater illuminance in offset direction of projection lens and modulator
- 55 9.037.469 T Automated communication integrator
- 56 9.014.322 **T** Low power and compact area digital integrator for a digital phase detector
- 57 9.009.697 T Hybrid cloud integrator
- 58 8.995.061 T Speckle reduction using lenslet integrator
- 59 8.988.904 T Power supply with integrator for controlling current
- 60 8.957.363 I Differential photodiode integrator circuit for absorbance measurements
- 61 8.952.749 T Filter with combined resonator and integrator
- 62 8.941.526 T Time integrator and .DELTA..SIGMA. time-to-digital converter
- 63 8.937.567 T Delta-sigma modulator, integrator, and wireless communication device
- 64 8.922.290 Pulse width modulator with two-way integrator
- 65 8.866.532 Passive integrator and method
- 66 8.866.531 **T** Broadband analog radio-frequency integrator
- 67 8,860,491 T Integrator output swing reduction technique for sigma-delta analog-to-digital converters
- 68 $8,854,107$ **T** Integrator circuit with inverting integrator and non-inverting integrator
- 69 8.851.684 Il Optical unit including an integrator optical system, and projection display device including the optical unit
- 70 8.835.827 T Current integrator with wide dynamic range
- 71 8.824.626 Reduced-noise integrator, detector and CT circuits
- 72 8.816.763 T Integrator input error correction circuit and circuit method
- 73 8,779,831 T Integrator July 2014
	- 74 8.775.003 T Methods and systems for controlling a proportional integrator
	- 75 8,767,343 T Disk drive increasing integrator output range to complete seek operation
	- 76 8.724.080 ^T Optical raster element, optical integrator and illumination system of a microlithographic projection exposure apparatus
	- 77 8,704,580 Circuit sharing time delay integrator
	- 78 8.674.864 T Integrator and oversampling A/D converter having the same
	- 79 8.665.129 T Complex second-order integrator and oversampling A/D converter having the same
	- 80 8.659.343 ^T Calibration for mixed-signal integrator architecture
	- 81 8,653,867 T Pulse modulated neural integrator circuit and associated phase locked loop
	- 82 8.639.513 T Automated communication integrator
	- 83 8.638.420 T Optical integrator, illuminating optical device, exposure apparatus and device manufacturing method
	- 84 8,614,639 T Integrator ramp generator with DAC and switched capacitors
	- 85 8.611.013 ^T Optical integrator, illumination optical device, aligner, and method for fabricating device
	- 86 8.587.764 T Optical integrator system, illumination optical apparatus, exposure apparatus, and device manufacturing method
	- 87 8.575.988 Mixed-signal integrator architecture
	- 88 8.573.779 I Lighting device with plural light sources illuminating distinct regions of integrator
	- 89 8.566.277 II System integrator and method for mapping dynamic COBOL constructs to object instances for the automatic integration to object-oriented computing systems
	- 90 8,564,358 T Integrator circuit with multiple time window functions
	- 91 8.558.610 T Integrator input error correction circuit and circuit method
	- 92 8.536.923 T Integrator distortion correction circuit
	- 93 8.526,487 T Differential energy difference integrator
	- 94 8,520,307 ^T Optical integrator for an illumination system of a microlithographic projection exposure apparatus
	- 95 8.504.503 Pulse modulated neural integrator circuit
	- 96 8.497.977 T Optical integrator, illumination optical system, exposure apparatus, and device manufacturing method
	- 97 8,438,201 Digital fractional integrator
	- 98 8.432.150 T Methods for operating an array column integrator
	- 99 8,432,149 T Array column integrator
	- 100 8,422,018 ^T Optical measurement apparatus including hemispherical optical integrator

Oct 16 2012
PAT. NO. Title

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- 1 8,290,897 T System integrator and method for mapping dynamic COBOL constructs to object instances for the automatic integration to object-oriented computing systems
- 2 8,283,966 T Integrator circuit
- 3 8,275,307 Vehicle audio integrator
- 4 8,264,388 T Frequency integrator with digital phase error message for phase-locked loop applications
- 5 8,258,990 T Integrator, resonator, and oversampling A/D converter
- 6 8.253.473 \blacksquare Integrated circuit of an integrator with enhanced stability and related stabilization method
- 7 8,199,038 T Active resistance-capacitor integrator and continuous-time sigma-delta modulator with gain control function
- 8 8.164.873 T Integrator and circuit-breaker having an integrator
- 9 8.145.597 If System integrator and method for mapping dynamic COBOL constructs to object instances for the automatic integration to object-oriented computing systems
- 10 8,129,972 \mathbf{T} Single integrator sensorless current mode control for a switching power converter
- 11 8,125,262 T Low power and low noise switched capacitor integrator with flexible input common mode range
- 12 8,098,377 T Electric gated integrator detection method and device thereof
- 13 8.081.098 T Integrator, delta-sigma modulator, analog-to-digital converter and applications thereof
- 14 8,035,439 \blacksquare Multi-channel integrator
- 15 8,031,404 T Fly's eye integrator, illuminator, lithographic apparatus and method
- 16 8.029.144 Color mixing rod integrator in a laser-based projector
- 17 8.028.304 Component integrator
- 18 8,013,657 T Temperature compensated integrator
- 19 8.011.810 T Light integrator for more than one lamp
- 20 7,997,740 T Integrator unit
- 21 7,965,795 ^T Prevention of integrator wind-up in PI type controllers
- 22 7,965,151 Pulse width modulator with two-way integrator
- 23 7,954,962 T Laser image display, and optical integrator and laser light source package used in such laser image display
- 24 7.943.893 I Illumination optical system and image projection device having a rod integrator uniformizing spatial energy distribution of diffused illumination beam
- 25 7,933,812 ^T System integrator and commodity roll-up

Apr 26 2011

- 26 7.932.960 T Integrator array for HUD backlighting
- 27 7.911.256 \blacksquare Dual integrator circuit for analog front end (AFE)
- 28 7.907.115 T Digitally synchronized integrator for noise rejection in system using PWM dimming signals to control brightness of cold cathode fluorescent lamp for backlighting liquid crystal display
- 29 7,905,631 T Illumination system having coherent light source and integrator rotatable transverse the illumination axis
- 30 7.884.662 T Multi-channel integrator
- 31 7.880.969 T Optical integrator for an illumination system of a microlithographic projection exposure apparatus
- 32 7,873,223 Cognition integrator and language
- 33 7,834,963 **T** Optical integrator
- 34 $7,830,197$ \blacksquare Adjustable integrator using a single capacitance
- 35 RE41,792 Controllable integrator
- 36 7,788,309 T Interleaved comb and integrator filter structures
- $377.773.730$ Voice record integrator
- 38 7.729.577 T Waveguide-optical Kohler integrator utilizing geodesic lenses
- 39 7.726,819 $\mathbf T$ Structure for protecting a rod integrator having a light shield plate with an opening
- 40 7.724.063 T Integrator-based common-mode stabilization technique for pseudo-differential switched-capacitor circuits
- 41 7.714.634 Pseudo-differential active RC integrator
- 42 7,706,072 ^T Optical integrator, illumination optical device, photolithograph, photolithography, and method for fabricating device
- 43 7,696,913 T Signal processing system using delta-sigma modulation having an internal stabilizer path with direct output-to-integrator connection
- 44 7.693,430 T Burst optical receiver with AC coupling and integrator feedback network
- 45 7.679.540 T Double sampling DAC and integrator
- 46 7,671,774 T Analog-to-digital converter with integrator circuit for overload recovery
- 47 7,658,497 Rod integrator holder and projection type video display
- 48 7,629,917 T Integrator and cyclic AD converter using the same
- 49 7.619,550 T Delta-sigma AD converter apparatus using delta-sigma modulator circuit provided with reset circuit resetting integrator
- 50 7,611,246 \blacksquare Projection display and optical integrator

Nov 3 2009

- 7.324.654 T Arbitrary coverage angle sound integrator 76
- 7,324,025 T Non-integer interpolation using cascaded integrator-comb filter
- 7,315,268 T Integrator current matching
- 7,304,592 T Method of adding a dither signal in output to the last integrator of a sigma-delta converter and relative sigma-delta converter
- 7,280,405 T Integrator-based current sensing circuit for reading memory cells 80.
- 81 7.262.056 Enhancing intermolecular integration of nucleic acids using integrator complexes
- 82 7.243.844 Point of sale integrator
- 83 7.242.333 T Alternate sampling integrator
- 84 7,205,849 Phase locked loop including an integrator-free loop filter
- 85 7,187,948 Personal portable integrator for music player and mobile phone
- 7.182.468 T Dual lamp illumination system using multiple integrator rods 86
- 87 7,180,357 \blacksquare Operational amplifier integrator
- 88 7.170,959 T Tailored response cascaded integrator comb digital filter and methodology for parallel integrator processing
- 89 7,155,470 Variable gain integrator
- 90 7.152.981 Projection illumination system with tunnel integrator and field lens
- 91 7,152,084 Parallelized infinite impulse response (IIR) and integrator filters
- 92 7,150,968 F Bridging INtegrator-2 (Bin2) nucleic acid molecules and proteins and uses therefor
- 7.138.848 Switched capacitor integrator system 93.
- 94 7.130.764 T Robust DSP integrator for accelerometer signals
- 95 7,102,844 T Dual direction integrator for constant velocity control for an actuator using sampled back EMF control
- 96 7,102,548 T Cascaded integrator comb filter with arbitrary integer decimation value and scaling for unity gain
- 97 7.098.845 **T** Apparatus for generating an integrator timing reference from a local oscillator signal
- 98 7.098.827 Integrator circuit
- 99 7,098,718 T Tunable current-mode integrator for low-frequency filters
- 100 7.087.881 ^T Solid state image pickup device including an integrator with a variable reference potential

Aug 8 2006

Jan 1976

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End of Lecture 23